ELEKTOR
1977 ISSUES

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What is a TUN? What is 10 kHz?
What is the EPS service?
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What is a missing link?

Semiconductor types
Very often, a large number of equivalent semiconductors exist with different type numbers. For this reason, 'abbreviated' type numbers are used in Elektor wherever possible:
• "741" stands for μA741, LM741, MC741, KM741, SN74741, etc.
• "7199" or 'TUN' (Transistor, Universal, PNP or NPN respectively) stands for any low frequency silicon transistor that meets the following specifications:

<table>
<thead>
<tr>
<th>Effect</th>
<th>Voltage</th>
<th>Current</th>
</tr>
</thead>
<tbody>
<tr>
<td>UCEO, max</td>
<td>20V</td>
<td>IC, max</td>
</tr>
<tr>
<td>hfe, min</td>
<td>20</td>
<td>Pot, max</td>
</tr>
<tr>
<td>ft, min</td>
<td>100 MHz</td>
<td></td>
</tr>
</tbody>
</table>

• "DUS" or 'DUG' (Diode Universal, Silicon or Germanium respectively) stands for any diode that meets the following specifications:

<table>
<thead>
<tr>
<th>Effect</th>
<th>Voltage</th>
<th>Current</th>
</tr>
</thead>
<tbody>
<tr>
<td>URS, max</td>
<td>25V</td>
<td>IF, max</td>
</tr>
<tr>
<td>IR, max</td>
<td>10μA</td>
<td>Pot, max</td>
</tr>
<tr>
<td>CD, max</td>
<td>5pF</td>
<td>10pF</td>
</tr>
</tbody>
</table>

Some 'DUS's are: BA127, BA217, BA218, BA221, BA222, BA317, BA318, BAX13, BAY61, 1N914, 1N4148. Some 'DUG's are: OA85, OA91, OA95, AA116.
• "BC107", "BC278", "BC547" all refer to the same "family" of almost identical better-quality silicon transistors. In general, any other member of the same family can be used instead.

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Printed in the Netherlands.
It is generally agreed that, as far as sound quality is concerned, moving-coil pickup cartridges have the edge over their moving-magnet counterparts. The moving-coil preamp design presented here can be built for around one-tenth the cost of a comparable commercial unit.

p. 4-02

Low cost, high transmission rate and complete reliability were the design requirements for the cassette interface described in the following article. The interface makes very few demands on the sound quality of the recorder, and can transfer data at a rate of up to 1200 Baud.

p. 4-20

An orchestra suddenly begins to recite a passage of Shakespeare, an electric guitar reads the news, the voice of a talker unexpectedly changes sex, a single voice sounds like a chorus — these are just a few of the amazing effects which can be obtained with a new electronic instrument — the vocoder. This article explains the ins and outs of this fascinating new development in the field of electronic ‘music’.

p. 4-27

The uncommon design approach used in the moving coil preamp is reflected in the repetitive nature of the printed circuit board!
General purpose active filter

Due to the previous successes of the AF100 Bi-Quad active filter and the AF120 Gyrator, National Semiconductor has introduced two new standard 'building block' filters, the AF150 and AF151.

The AF150 is a high frequency version of the AF100. Whereas the AF100 is limited to an upper frequency of 10 kHz and a center frequency - Q product of 50,000, the new AF150 has extended the upper frequency range to 100 kHz and center frequency - Q products to 200,000. This has been accomplished by using high frequency operational amplifiers and laser trimmed resistors.

Like its low frequency brother, the AF150 is a Bi-Quad configuration and offers extremely low sensitivity to external component changes. It simultaneously provides low pass, high pass and bandpass outputs while requiring only four external resistors to independently set the frequency, Q, and gain of the filter. In addition, by using an external operational amplifier, the LF356, all pass and notch filters can be formed.

Another new device, the AF151 is a dual Bi-Quad filter; that is, it provides two separate Bi-Quad active filters in one package. The performance of each filter section is identical to that of the AF100. This allows the user to easily design fourth-order filters in a single package.

In fact, because the package also contains two uncommitted operational amplifiers that can be used as buffers, summing amplifiers or elsewhere in the system, a really clever designer could make use of these amplifiers to design up to eight order filters in a single package. For example, one AF151 could be used for the transmit filter and one AF151 could be used as the receive filter in an asynchronous modem. It could easily be made to switch between originate and answer modes.

It appears that most filter being synthesized using Bi-Quad filters are of fourth-order and higher. For this reason it was decided to put it all in one package to offer the user lower manufacturing costs which are attendant with package insertion and smaller P.C. board space.

'The active filter revolution maybe analogous to the opamp revolution. As with an opamp, the user can simply put a few resistors around it and it does a specific job. It's a general purpose device, easily tailored, and saves P.C. board space, design time and money'.

There are thousands of uses for these filters. Once the designer establishes the center frequency, Q and gain requirements, a complicated sixth order filter design will normally take less than half an hour.

National Semiconductor GmbH
Industriestraße 10
D-8080 Fürstenfeldbruck
West Germany

Electronic shredder

The electronically sensing Fordshred 1800 represents a major advance in shredder technology. In addition to a power overload cut-out sensor, the 1800 features a unique electronic sensing device for paper load control. If the shredder is overloaded, the electronic sensor detects this before jamming occurs. The offending material is then rejected for separation and reintroduction. This means the operator can leave the machine unattended, secure in the knowledge that it will deal safely and efficiently with any prospective overload.

The Fordshred 1800 is precision-engineered and robustly built to take the strain of constant heavy duty shredding in commercial or industrial environments. Suitable for centralised operation, the powerful 1800 has an 18¼" wide throat and a voracious appetite, shredding cardboard and paper waste into ½″ strips at the rate of ½ ton per hour of continuously fed paper. Operating from a standard 13 amp power point, and working at a speed of 60 ft per minute, the machine will shred a complete file of some 50 sheets - including staples, pins and paper clips - in one pass! Destroyed material is simply ejected beneath the machine into a polythene sack. The sack is securely mounted on runners and, when full, can be slid out and replaced with a new one in seconds.

The 1800 is also an excellent machine for turning waste into profit by recycling waste paper to produce good quality packaging material for internal use or resale.

The machine is mounted on a rigidly constructed stand with four rubber-wheeled castors for complete mobility: the front two castors are fitted with brakes so that the shredder will remain completely stable whilst in use. To aid the operator further, the 1800 can be supplied with either a feeding shelf and side table for storing material prior to shredding or with a large work shelf for sorting loads.

The control panel, which faces the operator while the machine is in use, has well-spaced out, colour coded, 'forward' 'reverse' and 'stop' buttons. For added safety a master key is required to switch on the power. Conforming to BS 4644 and BS 3861 specifications for electrical and mechanical standards, the 1800 is powered by a ½ hp motor and operates on standard single phase 13 amp electricity supply. It measures 790 mm x 590 mm x 1092 mm high including stand (31" x 23" x 43"). The price is £ 1400 excluding VAT.

Fordigraph Division of Ofrex Limited,
Ofrex House, Stephen Street,

Semiconductors take over from TWTs

The Austrian Broadcasting Corporation (ORF) has replaced a total of ten travelling-wave-tube (TWT) amplifiers in five major transmitting stations by solid-state amplifiers of the type VD 100 from Rohde & Schwarz. Both technical and economic considerations played a role in the decision to reequip the low-power stages of the Band IV/V TV transmitters for the second program.

At about 400 VA each, the power consumption of the solid-state amplifiers is low compared with the 3 KVA of a TWT stage. The costs of the transition will be covered in about two years by the elimination of the tube replacement costs. With a gain of > 30 dB and a bandwidth of 470 to 860 MHz, the VD 110 provides the same functional performance as its predecessor.
moving coil preamp

In these days of laser scanners and microcomputers the mechanical process of a stylus being wiggled about in grooves, which have been scratched out of plastic to resemble the shape of sound waves, seems an incredibly crude and old-fashioned system. If it appears remarkable that such a process has continued in widespread use right up to the present day, it is even more remarkable that what could be described as such a conceptually primitive method allows sound to be reproduced with such startlingly good quality.

Innumerable constructional improvements have ensured that the record player has kept pace with the ever-increasing demands placed upon the fidelity of audio equipment. Better motors, improved drive systems, lighter and higher compliance pickup arms, the introduction of anti-skating compensation, and last but not least, a considerable improvement in the performance of pickup cartridges are all steps in the evolution of the old acoustic gramophone into the modern hi-fi record player.

This process of continual improvement is still evident, although it is now considerably less dramatic than in the past. The comparatively recent advent of direct-drive and crystal-controlled turntables are ample illustration. However as far as the domestic user is concerned, the latter innovation for example, can be counted among the category of snob-value 'improvements' which, although measurable, are audibly undetectable.

And it is a somewhat regrettable fact that a number of similar developments are designed more to stimulate sales than improve the user's appreciation of the reproduced sound.

Nonetheless, leaving aside such commercially-inspired innovations, there are still many areas where useful improvements in the audio chain can be made, and one which has — justifiably — received recent attention is the pickup cartridge.

A commendable development in this respect has been the trend to view the cartridge and pickup arm as a single unit, recognising the fact that one cannot assess the performance of the one without taking the other into account as well. A happy consequence of this has been the realisation that an extremely high compliance and an almost impractically low tracking force are not necessarily a prerequisite for top class cartridges.

Possibly these considerations have gained ground due to the increasing acceptance of the view among designers and reviewers of hi-fi equipment that, in addition to all the sophisticated electronic test equipment currently available, we possess two highly advanced but extremely inexpensive measuring devices in the form of our ears! This is a trend which cannot be welcomed too strongly, since ultimately, the assessment of any link in the audio chain must be determined not by specifications, distortion figures and the like, but by the subjective, if informed, response of the listener.

Moving coil cartridges

The above tendency provides a partial explanation for the recent increase in the popularity of moving coil cartridges. Although in the past they have been accused of poor tracking ability, and suffered from the disadvantage that they have to be returned to the manufacturer for stylus replacement, as well as being comparatively expensive, there has never been any doubt about the musical quality of moving coil pickups.

---

### Specification

- **Frequency response:** 7 Hz to 80 kHz, +0, −3 dB
- **Voltage gain:** 33.5 dB (1)
- **Input impedance:** 75 Ω (1)
- **Output impedance:** < 100 Ω
- **Recommended load:** 47 k
- **Impedance:**
  - **Maximum input voltage:** 23 mV
  - **Total harmonic distortion for Vm = 4 mV:** < 0.05%
  - **Channel separation:** < 60 dB
  - **Signal-to-noise ratio:** > 68 dB (2)
  - **Supply voltage:** 10 ... 20 V
  - **Current consumption (stereo version):** 100 mA

### Notes

1. Adjustable
2. Reference level is the output voltage produced using an Ortofon MC-20 cartridge tracking at 10 cm/sec.
While top-class cartridges of both moving-magnet and moving-coil types are capable of excellent performance, the sound of a moving-coil cartridge possesses a clarity and transparency not obtained from moving-magnet types. Thus many reviewers were inclined to have mixed feelings about this type of cartridge, since listening tests often gave much better results than could be expected on the basis of measured performance.

The question which no doubt most prospective buyers will ask, namely whether moving coil pickups are better than moving magnet types, fortunately does not fall within our brief. Indeed this is a question to which even reviewers of hi-fi equipment cannot really be expected to provide a generally valid reply, since the sound quality will be assessed differently by each reviewer.

A distinctive feature of moving coil pickups is the exceptionally direct and clear reproduction, which tends to distinguish them from their moving magnet colleagues. However there are top-quality moving magnet cartridges which often seem to possess just the right character for particular listeners, so that the serious audiophile should always take the trouble to compare different types of cartridges before making a purchase.

Unfortunately however, an effective comparison of different types of pickup is not always possible, since a moving coil cartridge produces an output voltage that is only a fraction of that produced by a moving magnet type. Thus to the not inconsiderable price of a moving coil cartridge has to be added the cost of a step-up transformer or—preferably, in view of its higher fidelity and lower sensitivity to hum—that of a special preamplifier. A suitable transformer will cost around £15, whilst a preamplifier could cost anything between £50 and £80—sufficient reason for many prospective users to settle for a moving magnet cartridge.

It is clear therefore that a powerful argument exists for building a suitable preamp oneself, thereby obviating the need to sacrifice one's musical discrimination for reasons of cost.

Preamplifier

Building a good preamplifier for very low signal levels is no easy matter, and the output signal of a moving coil pickup is extremely small indeed. Ortofon cartridges (which we have taken as a reference, since they have about the lowest output signal and since Ortofon is the only manufacturer of pickups who also produces a separate preamplifier) deliver approximately 70 µV per channel at an output impedance of 2 Ω. Thus a gain of around 50 would be required to boost this to the output level of an average moving magnet cartridge. It is clearly a tricky task amplifying such minute signals whilst maintaining an acceptable signal-to-noise ratio. By acceptable we mean a figure of at least 65 dB.

There are only a limited number of possibilities for the design of a suitably linear and low-noise preamp. One could look for an ultra-low-noise semiconductor. However, such a transistor would almost certainly be exorbitantly expensive, whilst availability would also present a thorny problem. Thus this approach does not seem very promising for a do-it-yourself type of project.

The alternative is to construct a simple but inherently low-noise amplifier stage and then see which readily available transistors give the best noise figure. Once this has been ascertained, the circuit is optimised for this particular transistor. Then a number of these amplifier stages are connected in parallel, as shown in figure 1. This trick was already explained in the article on the noise cancelling preamp which was published in last year's Summer Circuits issue (Elektor 27/28, circuit 75). If n identical amplifiers are connected in parallel then as far as voltage gain is concerned they will
function as a single amplifier, since each is fed with the same input signal, and each has the same gain. The outputs of all the amplifiers are thus equal and in phase. The noise voltages generated by the individual amplifiers, however, are random and, in mathematical terms, are uncorrelated with one another. Partial cancellation of the noise voltages will therefore occur at the amplifiers' common output. The result is that the signal-to-noise ratio of the output signal is effectively increased by a factor of \( \sqrt{n} \), where \( n \) is the number of amplifier stages connected in parallel.

In the case of this circuit, which contains eight amplifier stages, this means an improvement in the signal-to-noise ratio of 9 dB. To connect more than 8 stages in parallel is not considered worthwhile, since with such an arrangement the law of diminishing returns is applicable: to obtain a further (audible) improvement of 3 dB would require eight extra stages, and so on.

The circuit

The most obvious feature in the circuit diagram shown in figure 2 is the chain of amplifiers T1 .... T8. Although this arrangement may offend the aesthetic sensibilities of some readers, the resultant signal-to-noise ratio (> 68 dB!) testifies to its efficacy.

After some experiment, a reasonably cheap and commonly available transistor was found for the input stages: the BF494. It may seem a surprising choice at first sight, since this transistor is normally used in high frequency circuits. However the BF 494 is much more accustomed to handling very small input signals, and in fact proved more suited to this application than the members of, e.g., the BC family of transistors.

Additional voltage gain is provided by T9, and emitter-follower T10 acts as a low impedance output buffer capable of driving the relatively low-impedance feedback loop as well as the recommended output load. R21, R22 and C19 form the negative feedback loop, the mid-band gain being given by the equation

\[
\Lambda = 1 + \frac{R_{22}}{R_{21}}
\]

With the component values given, the mid-band gain is exactly 48. This is almost exactly the figure needed to boost the output voltage of an Ortofon moving coil pickup to the level of approx. 3.5 mV, which is the average output level of a moving magnet cartridge.

If one has a moving coil cartridge with a greater output voltage (Denon cartridges have an output roughly 4 times greater than average moving coil pickups), then the value of R22 can be increased to

Note: for stereo version, two of each required.

Resistors:
- (preferably metal film)
- R1 = 82 Ω
- R2 ... R9 = 18 k
- R10 ... R17 = 6k8
- R18 = 68 k
- R19 = 270 k
- R20, R23 = 470 Ω
- R21 = 47 Ω
- R22 = 1 Ω

Capacitors:
- C1 = 22 n
- C2 ... C9 = 470 µ/3 V
- C10 ... C17 = 4µ/10 V
- C18 = 4n7
- C19 = 33 n
- C20 = 47 µ/10 V
- C21 = 470 µ/10 V
- C22 = 100 n

Semiconductors:
- T1 ... T8 = BF 494 (BF 194, BF 195, BF 495)
- T9 = BC 560C, BC 559C, BC 179C or equiv.
- T10 = BC 547B, BC 107B or equiv.

Note: only one of each required.

Resistors:
- R24 = 1k5
- R25 = 6k2
- R26 = 1k2
- R27 = 1 k
- R28 = 100 Ω
- R29 = 8Ω2

Capacitors:
- C23 = 100 µ/10 V
- C24 = 1 n
- C25 = 4µ7/40 V

Semiconductors:
- IC1 = 723 (µA723, LM723, etc.)
- T11 = BD 241 (fitted with heat sink)
- D1, D2 = 1N4001

Parts to figure 3 and 4.

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Resistors:
- R1 = 82 Ω
- R2 ... R9 = 18 k
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- R18 = 68 k
- R19 = 270 k
- R20, R23 = 470 Ω
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- R22 = 1 Ω

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- T10 = BC 547B, BC 107B or equiv.

Parts list to figure 2 and 4.

Note: only one of each required.

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- T11 = BD 241 (fitted with heat sink)
- D1, D2 = 1N4001
2.2 Ω. This reduces the gain by more than half, so that there is no danger of overloading the disc input of the succeeding audio amplifier.

The input impedance of the amplifier is fairly low, and is largely determined by the value of R1. With the value given in the circuit diagram (R1 = 82 Ω) the input impedance exactly coincides with the recommended load impedance for the Ortofon moving coil pickup of 75 Ω. Other input impedances can be obtained by altering the value of R1 accordingly.

Power supply

The stereo version of the preamp requires a supply voltage of 6 V at 100 mA. This is supplied by a 723 IC voltage regulator with external transistor, as shown in figure 3. The regulator circuit requires an input of between 10 and 20 V at 100 mA. It may be possible to obtain this voltage from some existing piece of equipment such as an audio amplifier or preamp, but if such a voltage is not available then it must be provided by a separate transformer, bridge rectifier and smoothing capacitor. The transformer should have an RMS output voltage between 9 and 15 V at 160 mA and the bridge rectifier and capacitor should be rated at 30 V 100 mA and 220 μ (minimum) 25 V respectively.

Construction

Figure 4 shows a printed circuit board which will accommodate a stereo version of the preamp plus the supply stabiliser. It goes without saying that the components used in the construction must all be of the highest quality, otherwise the s/n ratio may be degraded. Metal-film and metal-oxide types are to be preferred for the resistors, and tantalum types are preferred for the capacitors. The transistors should have the mark of a reputable manufacturer, and if possible the 16 input devices should all be from the same production batch.

As the signal levels in the circuit are extremely low, a great deal of care must be taken in the construction. The printed circuit board must be housed in a totally screened (metal) case, and all signal lines should be of low-noise screened cable. To avoid earth loops the input socket(s) should be insulated.
**electronic input selector**

In most audio amplifiers the input selector switch is mounted on the front panel of the equipment, whilst the input sockets are mounted on the back panel. This means that the input signal leads must be routed all the way from the back panel to the front panel before going off to the actual amplifier input, thus increasing the possibility of hum and noise pickup crosstalk.

The transistor input selector described here switches the signals at the rear of the amplifier close to the input sockets. Switching is still controlled from the front panel switch, but audio signals no longer flow through it.

One channel of the selector is shown in Figure 1. Each input is fed to an emitter follower whose base bias voltage is obtained from the selector switch S1. When a particular input is selected by S1 then the appropriate transistor receives a base bias voltage and is able to pass the input signal. The bases of all the other transistors are pulled down to ground by resistors $R_B$ and are thus cut off.

Since S1 supplies only a DC bias voltage to the selector circuit the length of lead between S1 and the input selector is unimportant. An additional bonus is that the transistors function as impedance converters. The low output impedance means that there is no restriction on the length of lead between the output of the selector circuit and the input of the amplifier. Switching clicks are also suppressed since capacitors $C_2$ create the base voltages to die away smoothly rather than switching the transistors abruptly as S1 is operated.

The circuit can be extended to any number of inputs and any number of channels simply by adding an extra transistor for each additional input and duplicating the total selector circuit for each additional channel required.

**Testing**

The preamp should work immediately when it is switched on and a suitable signal is fed in. In the unlikely event of a fault occurring, however, the test point voltage shown in Figure 2 should be checked. Furthermore the collector voltages of transistors T1 to T8 should be approximately 1V. If the collector voltage of one (or more) transistors is significantly different from the rest then it is best to replace the offending device, since it will probably exhibit different characteristics from the other devices, which could have a detrimental effect on the s/n ratio.

Apart from this, provided care is taken in the construction, no problems should be encountered and the preamp should deliver a performance which compares favourably with that of commercial designs costing many times more.

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**Figure 5.** Photograph of the completed prototype, with the cover removed.

**Figure 6.** Another view of the prototype with the cover in place. In view of the low input signal levels, gold-plated phono connectors are recommended for the input sockets.

---

**Specification**

<table>
<thead>
<tr>
<th>Impedance of each input</th>
<th>$100 , \Omega$</th>
</tr>
</thead>
<tbody>
<tr>
<td>Maximum input voltage</td>
<td>$1 , \text{V RMS}$</td>
</tr>
<tr>
<td>Gain</td>
<td>$1 , \text{dB}$</td>
</tr>
</tbody>
</table>

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**Diagram**

- The diagram shows the electronic input selector circuit with components identified. The theory of operation and design considerations are described in the text. The preamp is designed to be a high-quality audio input selector with low input impedance, ensuring minimal signal degradation.

---

The preamp's design, with its use of high-quality components and thoughtful engineering, provides a robust and reliable solution for audio input selection, suitable for audiophiles and professionals alike.
There has been much debate in hi-fi circles about the necessity for high amplifier output powers, with some maintaining that a high output power is an absolute necessity for undistorted handling of programme peaks, and others maintaining that high-power amplifiers are just a status symbol. Be that as it may, there is no doubt that for many applications such as disco work, or situations where extremely inefficient loudspeakers are being used, a high power output is a definite advantage. With its choice of 50 W or 100 W maximum output power, the Elektronado should certainly satisfy most requirements.

A high output power either entails the use of a high supply voltage or the use of a bridge output stage. A bridge configuration was chosen for the Elektronado for several reasons:

1. It allows relatively inexpensive output devices to be used and avoids the necessity for expensive high-voltage (>60 V) devices.
2. Each half of a bridge amplifier can be used as an independent, lower power amplifier.

A bridge configuration entails the construction of two virtually complete amplifiers for each channel, so some way had to be found of reducing component count. Fortunately, the input and driver stages of the amplifier can be replaced by a single IC which has recently been introduced, the LM391. In the past, integrated circuits have not been very suitable for hi-fi applications due to limitations of bandwidth, distortion, noise and operating voltage. The LM391, however, suffers from none of these disadvantages.

The circuit

The complete circuit of one channel of the amplifier, including the equivalent internal circuit of the LM391, is shown in figure 1. The IC replaces all the input and pre-driver stages of the amplifier, the only parts of the circuit using discrete transistors being the driver and output stages.

The input stage of the IC consists of a differential amplifier (T1, T2) and a current mirror (T0, T3), which forms the collector loads for the differential stage. The signal from the collector of TH is fed to a cascode stage (T0, T3), which has a very high gain, and thence to the output stages of the IC.

The driver and output stages of the amplifier consist of two discrete transistor pairs T1/T3 and T2/T4, the quiescent current of the output stage being set by the collector/emitter voltage of transistor Tk, which is varied by adjusting the base bias by means of P1. To avoid distortion caused by slew-rate limiting (slope overload), care has been taken in the design of the feedback and compensation networks, and additional protection is provided in the form of an input filter R15/C11, which limits the slew-rate of the input signal. However, this does not have a detrimental effect on the normal frequency response, which begins to roll off at about 30 kHz.

The closed-loop gain of the amplifier is determined by the feedback network R5, R1 and C1. At frequencies where the reactance of C1 is small the gain is given by:

\[ AV = \frac{U_{out}}{U_{in}} = 1 + \frac{R_5}{R_1} \approx 22. \]

At low frequencies the increased reactance of C1 in series with R1 causes the gain to roll off to unity for DC signals. Amongst other things this avoids any DC offset problems which might result from a high DC gain. With the component values shown the voltage gain is approximately 20 (26 dB), which means that the input sensitivity for full output voltage swing is about 1 volt. This should make the circuit suitable for use with most modern preamps.

Circuit protection

Several protection circuits are incorporated into the design to prevent damage to the output transistors under various fault conditions.

Inductor L1, which is wound on R18, protects the output stage when operating into capacitive loads. Diodes D1 and D2 provide brute-force protection against any transients that might be produced by an inductive load by clamping the maximum output voltage excursion to ±U0.

A number of sophisticated protection circuits exist within the IC itself. Should
the output current of the amplifier rise above about 4 amps peak the voltage dropped across R12 or R13 will cause transistors T_L or T_M to turn on, thus limiting the output current.

Thermal protection of the output transistors may also be provided as an optional extra if desired. A negative temperature coefficient thermistor, which is in thermal contact with the output transistor heatsink, may be connected between pin 14 of the IC and ground. Current will flow through this thermistor via the two base resistors of T_A. As the temperature increases and the resistance of the thermistor falls this current will increase until the voltage drop across the 5 k resistor is sufficient to turn on T_A. This will shut down current sources T_B, T_C and T_D and cut off the drive to the output stage.

A resistor may need to be included in series with the thermistor to limit the maximum current out of pin 14 to 1 mA, and the thermistor value should be chosen such that the current out of pin 14 will be about 100 μA at the desired cutoff temperature.

**Two-channel amplifier**

Figure 3 shows the complete circuit of a two-channel amplifier. In this case, for simplicity, the internal circuit of the LM391 is not shown. With a ± 30V supply each channel of the amplifier will deliver 50 W into an 8 ohm load, or 45 W into a 4 ohm load. By connecting a resistor, R_X, between the output of one channel and the inverting input of the other channel (non-inverting input grounded) the two channels can be made to function as a mono bridge amplifier, with the loudspeaker connected as shown dotted. Note that in this configuration both ends of the loudspeaker are floating.

Theoretically, the maximum output power that can be obtained in the bridge mode is four times that obtained in the normal configuration. However, this would place great stress upon the output transistors and would require much more massive heatsinks and an extremely 'beefy' power supply. The maximum output power into an 8 ohm load in the bridge configuration is therefore restricted to 100 W by current limiting. Operation into a 4 ohm load in the bridge configuration is not recommended as current limiting will restrict the maximum output power to about 45 W.

**Printed circuit board**

The printed circuit board and component layout for the Elektornado are given in figure 4, and it will be seen that
two identical channels are mounted on a single board to facilitate operation in the bridge mode. If this configuration is required then $R_X$ is soldered into place and the input of the left channel is grounded. If the 2 x 50 W stereo version is required then $R_X$ is omitted.

$L_1$ consists of 20 turns of 0.9 mm (20 SWG) enamelled copper wire, wound on the body of resistor $R_{18}$.

The driver and output transistors are, of course, mounted external to the board on heatsinks, which should have a thermal resistance of less than $1.5^\circ C$ per watt and should be mounted with the fins running vertically to give a chimney effect which will aid cooling. Painting the heatsinks matt black also improves cooling.

**Wiring**

To avoid problems of instability, earth loops etc. the wiring layout shown in figure 5 should be followed. For clarity the driver and output transistors are not shown in this diagram. A simple, unstabilised power supply between ±15 V and ±30 V is quite adequate for the amplifier, although the maximum output power will only be obtained with the higher supply voltage. Care should be taken to ensure that the off-load voltage of the power supply is no greater than ±30 V, otherwise there is a danger of damaging the IC or output transistors. The $2 \times 20$ V RMS secondary rating of the transformer should be considered as an absolute maximum, as this will allow for a ±10% variation in mains voltage.

**Setting quiescent current**

Before applying power to the amplifier $P_1$ and $P_1'$ should be turned fully to the

---

**Figure 1.** Circuit of one channel of the Elektornado, showing the internal circuit of the LM 391 IC.

**Figure 2.** Pinning of the driver and output transistors (all bottom view).

**Figure 3.** Complete circuit of the 50 W per channel/100 W mono amplifier.

**Table 1.** Principal specifications of the Elektornado amplifier.
Parts list to figure 5.

Resistors:
- R1, R1', R4, R4' = 4 kΩ
- R2, R2', R5, R5', R6, R6', R9, R9', Rx = 100 kΩ
- R3, R3' = 47 kΩ
- R7, R7', R8, R8', R15, R15'
- R16, R16', R17, R17' = 1 kΩ
- R10, R10', R11, R11' = 100 Ω
- R12, R12', R13, R13' = 0.15 Ω/3 W
- R14, R14' = 10 Ω/1 W (carbon film resistor)
- R18, R18' = 1 Ω/1 W (carbon film resistor)
- P1, P1' = 10 kΩ preset

Capacitors:
- C1, C1' = 4 µF/16 V
- C2, C2' = 1 µF/63 V
- C3, C3', C6, C6' = 10 µF/63 V
- C4, C4', C7, C7' = 40 µF
- C5, C5', C10, C10', C13, C13', C14, C14' = 100 nF
- C8, C8', C9, C9', C11, C11' = 1 nF
- C12, C12' = 47 nF

Semiconductors:
- IC1, IC1' = LM 391-60 or LM 391-80
- T1, T1' = BD 139
- T2, T2' = BD 140
- T3, T3' = TIP 2955 or MJE 2955
- T4, T4' = TIP 3055 or MJE 3055
- D1, D1', D2, D2' = 1N4002

Figure 4. Printed circuit board and component layout for the Elektornado (EPS 9874).

Figure 5. Wiring diagram for the Elektornado (driver and output transistors not shown).

Figure 5a: stereo version; figure 5b: bridge version.

Figure 6. Total harmonic distortion versus frequency graph for the Elektornado.
left.

A multimeter set to the 100 mA range is then connected in the positive or negative supply lead to the left channel, and P1 is adjusted to give a current of between 50 and 100 mA. The procedure is then repeated for the right channel.

If the amplifier should exhibit any tendency to instability (this may manifest itself as an excessively large and uncontrollable quiescent current) this can be cured by increasing the values of C4 and C7, keeping them of equal value.

Conclusion

The specifications of the Elektornado can safely be called excellent. As can be seen from figure 6 the harmonic distortion is below 0.1% over the entire audio spectrum, and over the important mid-band frequencies is less than 0.02%. Other important parameters of the amplifier are listed in table 1.

As mentioned previously, the input sensitivity for full output is 1 V RMS, which should be suitable for most pre-amplifiers. However, if this sensitivity is insufficient the gain of the amplifier may be increased simply by changing the values of R1 and R5 (decreasing R1 and/or increasing R5).

The high output power and excellent specifications of the Elektornado, together with its versatility, should ensure that it will prove the right answer for a great number of amplifier applications.
Conventional rotary or slider potentiometers suffer from several disadvantages when used as volume controls in an audio system. The ganged, logarithmic potentiometers which are frequently employed in stereo amplifiers frequently suffer from poor matching of the two channels, so that the relative signal levels or balance of the left- and right channels vary as the control is operated. Carbon potentiometers also have a relatively limited life and soon become noisy in operation.

One solution to these problems is to use a stepped volume control consisting of a switched, resistive potential divider, as shown in figure 1. This circuit has several advantages over a conventional potentiometer:

- matching between channels is determined solely by resistor tolerances (5% tolerance should be adequate for most applications)
- the control can be made to have any desired 'law' by suitable choice of resistor values
- within reason, any number of channels can be catered for by using a switch with more wafers
- a long life is obtained, provided a reasonable quality switch is used.

The degree of attenuation produced for a particular setting of the control is given by attenuation = 20 log (Rf/Rt) dB, where Rf is the total resistance of the potential divider chain and Rt is the remaining resistance between a particular switch position and ground. The value of individual resistors connected between two adjacent positions of the switch is obviously obtained by subtracting two adjacent values of Rt.

For a volume control a logarithmic law is desirable, which means that the difference in attenuation between any two adjacent settings of the control must be a constant number of dB. Table 1 shows the values of Rt required for 1 dB steps of attenuation from 0 to -60 dB for an Rt value of 100 k (plus an extra step for infinite attenuation). Obviously a practical volume control cannot have this number of steps, as this would require a 62-way switch. On the other hand, the number of switch positions must not be too small, as this will not give sufficiently fine control.

Table 1

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A reasonable choice of attenuation step is 3 dB. This gives sufficiently fine control, yet allows 60 dB of attenuation to be achieved in 21 steps. Allowing an extra step for the zero (infinite attenuation) position means that 22 ways are required in all.

The resistance values for a 22 position control are given in table 2. Column 1 lists the required attenuation in dB for each switch position. Column 2 lists the corresponding values of RL. Column 3 lists the resistor values required between the switch positions. Column 4 lists the actual values used (made up from standard E24 series resistors). Column 5 lists the actual values of RL obtained and column 6 lists the actual values of attenuation obtained using these resistor values.

Resistor values for values of RL other than 100 k can be obtained simply by scaling the resistor values given. For example, for a 50 k control the values should all be halved, for a 10 k control they should be divided by 10 and so on.

One final point to note is that the switch contacts should be of the make-before-break type to avoid switching clicks as the control is operated.

---

**real load resistors**

When measuring and comparing the output powers of audio amplifiers (especially at the high end of the audio spectrum) it is useful to have available a 'real' load resistor, i.e. one which is a pure resistance with no parasitic inductance or capacitance. Carbon film resistors have a low self-inductance, but unfortunately are not commonly available in the high power ratings required for amplifier testing. The highest rating normally available in a carbon film resistor is 2 watts, so a load resistor for testing a 100 W amplifier would need to be made up of 50 such resistors in series/parallel combinations!

Wirewound resistors are available with high power ratings, but unfortunately such resistors are rarely wound so as to minimise self-inductance. A typical high-power wirewound resistor consists of a single layer of resistance wire wound helically on a cylindrical ceramic tube. This type of resistor has a high self-inductance, but since the usual applications of high-power wirewound resistors are DC or low-frequency AC this is not important.

---

For use as an amplifier load resistor some means must be found of reducing the inductance of a wirewound resistor. This can be achieved by providing the resistor with a centre tap and connecting it as shown in figure 1. Current flows in opposite directions in each half of the resistor, so the magnetic fields produced in each half (and hence the self-inductances) tend to cancel out. If the original resistor has a value R then the connection shown has a resistance R/4 since it consists of two R/2 sections in parallel.

Resistors already provided with taps, such as television H.T. dropper resistors, are suitable for this application. Presettable resistors may also be used. These consist of an exposed wire element wound on a ceramic former, and are provided with contact clips that may be fixed anywhere along the length of the element. 1 kW electric fire (heating) elements (which have a resistance of around 60 Ω) may also be used. In order to obtain a load resistor of the desired resistance and wattage rating, several wirewound resistors may be connected in series/parallel combinations in the normal way, provided each one is first connected as shown to minimise its inductance.
The dynamic range of an audio signal is the ratio, expressed in decibels (dB), between the largest and smallest usable signal levels, i.e., between the loudest and softest sounds. 'Live' sound, from the softest whisper to the clatter of a pneumatic drill, can have a dynamic range in excess of 100 dB. However, it is not possible to capture such a large dynamic range in a recording, since the largest signal that can be recorded is limited by saturation of the recording medium, and the smallest usable signal is limited by the recording medium's own inherent noise, e.g., tape noise or record surface noise. The ratio between these two, i.e., the dynamic range, is only about 60 dB for the best disc recordings, and considerably less (around 45 dB) for cassette recordings.

One way round the problem is to compress the dynamic range of the original programme material before recording it, i.e., to pass the signal through a system whose gain reduces progressively as the signal level increases. Thus a 2 dB change in signal level at the input could be compressed, for example, into a 1 dB change in level at the compressor output. To recreate the original dynamic range the compressed recording is 'expanded' by replaying it through a system having the reciprocal transfer characteristic of the compressor, e.g., a circuit which gives a 2 dB change in output for a 1 dB change in input level.

Disc to cassette
The dynamic range of material recorded on disc is compressed into the 60 dB dynamic range of this recording medium, but discs are normally played back without expansion since a dynamic range of 60 dB is considered adequate for domestic listening. Quite recently, DBX have introduced a disc compression/expansion system, but any expander system will, of course, add to the cost of disc reproduction equipment.

Transcribing discs onto cassette tape using a deck already equipped with a noise reduction system (Dolby, ANRS) is no problem. However, there are many inexpensive cassette decks on the market that are not equipped with a noise reduction system, and the results obtained when discs are recorded using such a machine are likely to be disappointing, since the dynamic range is inadequate. Recordings made taking care not to overload the tape will have excessive background noise on quiet passages, while recordings made to give a reasonable noise level on quiet passages will exhibit distortion due to overloading on loud passages.

Normally, the only way to improve matters is to control the dynamic range of the programme material manually during recording, by 'riding' the recording level control. This can be very tedious if long passages are to be recorded, so a simple expander would be a useful addition to an inexpensive cassette machine.

The XR 2216
Until recently expanders were fairly complex circuits, but fortunately a complete expander system is now available in the form of an integrated circuit from Exar – the XR 2216.

The equivalent circuit and functional block diagram of this IC are shown in figure 1. The device contains an AC/DC converter which converts the AC signal fed to it into a proportional DC control voltage, a voltage-controlled impedance converter (which functions as a voltage-controlled attenuator) and a high-gain operational amplifier.

Figure 2 shows the external components and circuit connections necessary to make the XR 2216 function as an expander. The input signal (from the tape deck, for example) is applied to pin 7, the input of the AC/DC converter, the output of which controls the transconductance of the impedance converter. The input signal is also fed to the impedance converter, the output of which is thus proportional to the product of the input signal and its average value from the AC/DC converter, i.e., the transfer function of the expander is a square law. The impedance converter output is fed to the operational amplifier by linking pins 11 and 16, and the expanded output signal is taken from pin 2.

By re-arranging the circuit slightly it can be
Table 1

**ELECTRICAL CHARACTERISTICS:** \( V_C = +12 \text{ V}, T_A = 25^\circ \text{C} \)

### COMPARATOR

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### COMPRRESSOR

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### EXPANDER

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<td>-37</td>
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Notes: * 0 dB = 0.775 Vrms (1 mW across 600 ohm load)  ** Recommended transfer characteristics.
be made to function as a compressor, the circuit of which is shown in figure 3. In this case the input signal is fed to the input of the impedance converter (pin 10) and from the output of this stage to the input of the operational amplifier, the output (to the tape deck) again being taken from pin 2. A portion of the output signal is fed to the input of the AC/DC converter, (by linking pins 2 and 7), the output of which again controls the transconductance of the impedance converter. In this case the output is thus proportional to the square root of the input signal, i.e. the transfer function is the reciprocal of the expander circuit's.

The attack and decay times of the circuit are equal and are determined by a filter consisting of an external resistor and capacitor (P1/C3 or P3/C8). It is important that the attack time should not be too long, otherwise the response of the circuits to transients may be too slow to prevent overload.

On the other hand, if the decay time is too short then ripple may appear on the output of the AC/DC converter at low input frequencies, thus leading to modulation of the output signal and third harmonic distortion. This is not a problem in a compander system, since the distortions produced in the compression and expansion processes tend to cancel out. However, if the circuit is used simply as a compressor or as an expander then distortion at low frequencies is a major problem.

Two preset adjustments are provided in the circuits of figures 2 and 3. P1 and P3 set the reference level of the circuit, which determines the actual input voltage range over which the compression/expansion takes place. P2 and P4 set the low level tracking, which ensures that the compression and expansion characteristics match, thus ensuring (amongst other things) minimum distortion.

Performance data

The specifications of the XR2216 are given in table 1, and typical performance curves in figure 4. It can be seen that, in the compressor mode the circuit provides a 2 : 1 compression ratio, e.g. a 60 dB dynamic range can be compressed into 30 dB. In the expansion mode, not surprisingly, an expansion ratio of 1 : 2 is obtained, thus restoring the original dynamic range.

From table 1 it can be seen that distor-
When making a sound recording using multi-microphone techniques the signal picked up by each microphone can be correctly positioned in the stereo sound stage by 'panning'. For example, the signal from a centrally placed microphone would be fed equally to both left- and right channels, a signal from a microphone located at the left of the sound stage would be fed only to the left channel and a signal from a microphone located at the right would be fed only to the right channel. Signals from microphones located between these positions would be fed to the left- and right channels in the appropriate proportions.

A circuit which allows the position of the sound image from a particular microphone to be positioned is known as a panoramic potentiometer or pan pot and usually consists of a ganged log-antilog potentiometer. The input signal is fed to both halves of the potentiometer and the left- and right outputs are taken from the wipers. Turning the potentiometer to the right increases the right channel level and decreases the left channel level, and vice versa.

Operation of a pan pot must not vary the total signal level, i.e. if the output level from the left or right channel with the pan pot in its extreme left- or right position (other channel muted) is taken as 0 dB, then the signal level from each channel with the pan pot central must be -3 dB to keep the total signal constant.

Figure 1 shows the circuit of a pan pot which uses only a single, linear potentiometer. The input signal from, say, a microphone preamplifier is split into two channels. The resistor and potentiometer values are chosen such that, with R1 in the extreme left position (wiper towards R1') the gain of the left channel is 1.066 whilst the right input signal is shorted to ground via the wiper of R1. With R1 in the extreme right position the reverse is true. With the wiper of R1 in its centre position the gain of both channels is 0.746, which is approximately 3 dB down on the gain in the extreme positions.

National Semiconductor appl.
723 as a constant current source

The µA 723 precision voltage regulator IC is well known for its versatility, good line and load regulation, and low temperature coefficient. In addition to its many uses as a voltage regulator, it can also be used as a precision current regulator (constant current source).

Figure 1 shows a simplified internal circuit of the µA 723, equivalents for which are the LM723 and TBA281. It contains a temperature-compensated voltage reference, a differential amplifier, driver and output transistors and a current sense transistor for current limiting purposes. A temperature-compensated reference voltage of 7.15 V +/- 5% is available at pin 4 (metal can version) or pin 6 (DIL package version). Familiarity with this internal circuit will aid in understanding the operation of the 723 as a constant current source, which is shown in figure 2.

The differential amplifier is connected as a voltage-follower, with the output $V_O$ fed directly back to the inverting input. A potential divider, $R_2/R_3$, connected across the reference voltage output, feeds a voltage of about 2.2 V to the non-inverting input. Since the differential amplifier is connected as a voltage follower, 2.2 V appears at output $V_O$. This causes a constant current

$$I = \frac{2.2}{R_1}$$

to flow through $R_1$. Since this current flows from the positive supply rail into the $V_C$ pin, it must also flow through the external load $R_L$. This current is constant, irrespective of the value of $R_L$, within certain limits. The maximum value of $R_L$ is given by:

$$R_L = \frac{U_B - 2.2}{I} \quad (\Omega, \text{V, A}).$$

Although the maximum output current capability of the 723 is 150 mA, care must also be taken not to exceed the 800 mW maximum dissipation of the IC. Maximum dissipation occurs when $R_L$ is zero, since almost all the supply voltage is then dropped across the output transistor of the IC. The dissipation is given by:

$$P = (U_B - 2.2) \times I \quad (\text{W, V, A}).$$

Rearranging this equation and substituting 0.8 W as the maximum dissipation, the maximum current that can safely be supplied (into a short-circuit) is

$$I_{\text{max}} = \frac{0.8}{U_B - 2.2} \quad (\text{A, W, V}).$$

With a 10 V supply this is approximately 100 mA, and with the maximum supply (37 V) it will be approximately 23 mA.

The 723 may be provided with a thermal shutdown facility to protect against overheating. This is achieved by using the current limit transistor in the IC as a temperature sensor. At 30°C the base-emitter 'knee' voltage of this transistor is about 0.65 V, but at 120°C it has fallen to about 0.5 V. Resistors $R_4$ and $R_5$ (shown dotted) apply approximately 0.5 V to the base of this transistor (note also the dotted connection to the $C_3$ terminal). This is normally less than the base-emitter knee voltage and is insufficient to turn on the transistor, but at 120°C, when the knee voltage has dropped to 0.5 V, the transistor will start to turn on. This will reduce the base drive to the IC's output stage, decreasing the output current and hence the dissipation.

If a larger output current is required than can be provided by the µA 723, an external power transistor may be added, as shown in figures 3 and 4. If an NPN transistor is used then it is simply connected as an extension of the emitter-followers in the IC's own output stage: base to $V_O$, emitter to the inverting input of the differential amplifier. However, if a PNP transistor is used a slight
723 as a constant current source

Figure 1. Simplified internal circuit of the 723 IC regulator. Numbers in parentheses are pinout of the DIL package version; others, pinout of the TO-metal can version.

Figure 2. The 723 used as a constant current source.

Figures 3 and 4. If a larger output current is required than can be provided by the 723 alone, an external NPN or PNP power transistor may be added.

The rearrangement of the circuit is necessary: $V_o$ and the inverting input are linked, and the base of the transistor is connected to $V_C$, the collector of the IC’s output transistor. The equation previously given for calculating the output current also holds for these two circuits.

The thermal shutdown facility may also be added to these circuits, but it should be emphasised that it will protect only the IC, not the external transistor. As the dissipation in the external transistor may be quite high it is essential to provide it with a substantial heatsink. For example, with a 37 V supply and a current of 1 A, the short-circuit dissipation in the external transistor will be about 35 W!
Low cost, high transmission rate and complete reliability were the design requirements for the cassette interface described in the following article. The interface makes very few demands on the sound quality of the recorder, and can transfer data at a rate of up to 1200 Baud.

FSK modulator
The FSK modulator uses a well-known IC function generator, the XR-2206 (see figure 2). The IC is powered by the two supply voltages already present in the SC/MP system, i.e. +5 V and −12 V. Transistor T1 is included so that the IC can be driven by TTL logic levels. The input and output signals of the modulator are shown in figures 5a and 5b, respectively. The amplitude of the output signal can be varied by means of P3, and hence adjusted to suit the input sensitivity of the particular tape recorder being used. The frequency of the output signal can be set to 1,200 Hz and 2,400 Hz by means of P1 and P2 respectively. This can be done either by using a frequency meter, or if that is not possible, by utilising the SC/MP clock generator.

Tuning the modulator
Since the SC/MP has an internal crystal clock generator, it is possible, with the aid of a short programme, to get it to generate signals whose frequency is remarkably constant. Table 1 shows the listing for such a programme. Once it has been loaded into memory and run, a squarewave signal with a frequency of either 1,200 Hz or 2,400 Hz is available at Flag (pin 14C of the connector bus). The actual frequency of the signal
depends upon the 'number' written into 'XX' and 'YY' (see table 1). These signals can then be used to tune the modulator as follows:

- Flag 0 and the modulator output are connected as shown in figure 3. A high impedance earphone or a tape recorder with input level meter is then connected to the output of the above circuit.
- The programme for the 1,200 Hz tone is started, and a logic '0' is presented to the modulator input (potentiometer P3 is set for maximum amplitude). Several different frequencies should now be audible in the earphone, namely the 1,200 Hz signal produced by the SC/MP, the tone produced by the modulator and the difference- or beat signal.
- P1 is adjusted until the beat signal frequency is reduced to a minimum, when the frequency of the modulator output should be virtually the same as that of the programme signal. If using a VU-meter then P1 is adjusted until the needle ceases to jitter.

The procedure for the 2,400 Hz signal is exactly the same, except that the SC/MP is programmed to produce a 2,400 Hz signal and a logic '1' is applied to the modulator input.

**FSK demodulator**

The circuit for the demodulator is considerably more complicated than that for the modulator. The complete circuit diagram of the FSK demodulator is shown in figure 4. Its operation differs from the conventional method of FSK demodulation (PLL), but the series of voltage waveforms shown in figure 5 should help to simplify its explanation.

The FSK signal (figure 5b) is fed to the
input of de demodulator, where it is clipped symmetrically by the limiter amplifier A1 (figure 5c) before being fed to a Schmitt trigger (N1, N2). The output of the trigger and its inverted form are each fed to a differentiating network (C9, R18 and C10, R19). The result is that a signal which has twice the frequency of the original input signal of the Schmitt-trigger is present at the collectors of T2 and T3 (see figure 5d). This signal is then used to gate a monostable multivibrator (M1). The output of the monostable is a train of pulses of constant width (figure 5e).

These pulses are fed to an integrating network (R22, C13), producing the signal shown in figure 5f. The voltage across capacitor C13 (figure 5f) can be used to monitor the frequency of the input signal, since the increase in charge per unit of time is twice as great in the case of the higher frequency (2,400 Hz) than in the case of the lower frequency (1,200 Hz). In order to convert this small difference in the DC component of the voltage across C13 into a digital signal, a sample-and-hold circuit (A2, T4 and C14) is used as a memory. A sample-pulse is derived from the output of M1 by means of a second monostable (M2). During this sample-pulse (figure 5g) the sample-and-hold circuit samples and then stores the instantaneous value of the voltage across C13. If the frequency of the demodulator input signal is constant, then the voltage at the output of the sample-and-hold circuit (= emitter of T4) will also be virtually constant. If the frequency of the input signal varies, then at the moment of sampling, the instantaneous value of the voltage across C13, and hence the output voltage of the sample-and-hold (figure 5h) will also vary.
Figure 4. The circuit diagram of the FSK demodulator.

Figure 5. Diagram of the various voltage waveforms at different points in the demodulator circuit.

Table 2. Programme for tuning the demodulator.

Although this output voltage is in fact a digital signal, its amplitude and logic voltage swing are not very large, and hence a comparator (A3 and N5, N6) is required to bring the signal up to TTL logic levels. The threshold voltage of this comparator in fact represents the only adjustment point in the entire demodulator, and once again a simple programme will prove useful.

Tuning the demodulator
If the demodulator is fed a 'symmetrical'
Parts list to figures 6 and 7

Resistors:
R1 = 1 k
R2 = 4 k
R3, R6, R18, R19, R23 = 12 k
R4 = 5k6
R5, R11, R13, R20, R21, R22, R26, R27 = 22 k
R7, R12, R24, R34 = 220Ω
R8, R9 = 10 k
R10 = 18 k
R14 = 15 k
R15, R28 = 100 k
R16 = 1 M
R17 = 1 k
R25 = 27 k
R29 = 220 k
R30 = 470 k
R31 = 2 k
R32 = 470 Ω
R33 = 3 M
P1 = 10 k
P2 = 5 k
P3 = 25 k
P4 = 1 k

Capacitors:
C1 = 27 n
C2, C3 = 10 μ/16 V
C4 = 1 μ/16 V
C5 = 180 n
C6 = 1 μ/8 V
C7 = 100 p
C8 = 56 n
C9, C10, C15 = 1 n
C11, C13 = 10 n
C12 = 150 p
C14 = 1 n
C16 = 47 n
C17 = 47 μ/6 V
C18, C19 = 100 n
C20 = 3 m

Semiconductors:
D1, D6 = 1 N4148
T1 = BC557, TUP
T2, T3 = BC547 TUN
T4 = BC517
IC1 = XR-2206
IC2 = CA3050
IC3 = 4049 (CD4049, etc.)
IC4 = 74123

Figure 6. Track pattern of the interface board (EPS 9905).

Figure 7. Component layout of the interface board.

Figure 8. Wiring diagram for the connections between the SC/MP system (bus board) and the cassette interface.
input signal, i.e. a signal consisting of equal-lengthed portions of 2,400 Hz and 1,200 Hz, then the output signal must also be symmetrical. Table 2 lists a programme which will generate a symmetrical input signal for the demodulator. This signal is available at Flag 0 of the SC/MP and hence the demodulator input should be connected to this point (connector pin 14C).

The output signal is adjusted by means of P4. Since a symmetrical signal which swings between supply and earth has an average value which is equal to half supply, the demodulator output should be connected to a DC voltmeter and P4 adjusted until a reading of 2.5 V is obtained. That completes the adjustment procedure for the demodulator.

Printed Circuit Board
A printed circuit board was designed to accommodate both the modulator and demodulator circuit. Figures 6 and 7 show the track layout and component overlay of the board. Once the components have been mounted and both circuits correctly adjusted, the board can be connected to the SC/MP system as shown in figure 8.
car rip-off protection

The complete circuit of the alarm is shown in figure 1. N1 to N4 form a 5-input OR gate, but the number of inputs can easily be increased by adding extra gates. When the car is unoccupied (and the ignition is switched off) R11 holds the inputs of N5 low, so the output is high. The inputs of N1 to N4 are held low via the filaments of the lamps, etc. that are being protected. The output of N4 is thus low, the output of N6 is high, T1 is turned on, T2 is turned off and relay Re 1 is de-energised.

In the event of an accessory being disconnected by a thief (for example, the lamp connected to input E1), then the appropriate input to the OR gate will be pulled high by the 10 k input resistor. The output of N4 then goes high, the output of N6 goes low, T1 is turned off and T2 is turned on, energising Re 1 and sounding the car horn.

When the ignition switch is closed the output of N5 is low, which holds the output of N6 permanently high, thus disabling the alarm. This prevents the alarm from sounding when one of the accessories is switched on. Of course, the alarm will still sound if an accessory is switched on whilst the ignition is switched off. This prevents spotlamps and foglamps from accidentally being left on whilst the car is unoccupied. Alternatively, these accessories can be wired via the ignition switch so that this cannot occur.

An additional bonus is that the alarm will also sound in the event of a lamp filament failure. However, since a replacement lamp may not always be available, a secret 'cancel' switch (S1) is required...

Accessories inside the car, such as radios and cassette players, may also be protected by connecting a wire from one of the alarm inputs to the earthed case of the equipment. When the thief cuts this wire to remove the equipment then the alarm will sound. Of course, this facility should only be regarded as a backup to an alarm that prevents a thief entering the car in the first place!

Where lamps are wired in pairs the alarm will, of course, not sound until both have been disconnected. To overcome this disadvantage a diode of suitable current rating can be wired in series with each lamp, as shown in figure 2a. Since there is a 0.7 V voltage drop across a diode, a better idea would be to use a double-pole switch for the set of lamps being protected, as shown in figure 2b.

Thefts from cars of valuable accessories such as spotlamps and foglamps are on the increase. Equipped with a spanner, and given a few minutes undisturbed, the enterprising felon can frequently make a haul worth over £100. The inexpensive alarm circuit described in this article will protect these valuable items, and can also be used to prevent the theft of accessories from inside the car, for example radios and cassette players.

W. Braun

Figure 1. Complete circuit of the car rip-off theft alarm.

Figure 2. Lamps connected in pairs must be isolated from one another, otherwise the alarm will not give complete protection. This can be done with a pair of diodes, as shown in figure 2a, or by double-pole switching, as shown in figure 2b.
A vocoder (VOice CODER) is an instrument designed to analyse and electronically recreate the sound of the human voice. Although vocoders are in fact a far from recent invention, and have been used for a number of years in such fields as telecommunications and data processing, it is only within the last couple of years that a serious attempt has been made to exploit their enormous potential for musical and sound effect applications.

History
The term ‘vocoder’ was first coined in 1936 by an American called Homer Dudley, who invented a machine to compress the bandwidth of speech for transmission purposes. There was also a certain amount of interest in vocoders in Germany during the thirties. This interest was stimulated by the realisation that they had an obvious military potential — the encoding of secret messages.

By the middle of the sixties Siemens possessed a vocoder which was occasionally used for recordings. Similarly the BBC Radiophonic Workshop, and a number of other experimental studios used vocoders for special effects on records, radio and television. However all these early prototypes suffered from the drawback of being extremely large and unwieldy, and as such were quite unsuited for other than specialised applications.

The real breakthrough came in 1975 with the appearance of a vocoder which, by virtue of its compact and ergonomical design, was suitable for use in a conventional studio situation where it could be interfaced with other equipment, thus allowing its full potential to be realised. This was the EMS (Electronic Music Studios) Vocoder (see photo 4) developed by Tim Orr, a self-contained portable instrument that can not only synthesise speech at constant and varying pitch, but by using a second non-speech input signal can encode literally any recorded sound with any speech sound.

The machine can thus produce the effect of ‘talking’ musical instruments. Since the EMS Vocoder, Sennheiser and other manufacturers have capitalised upon their experience of using vocoders in the field of telecommunications, and with the assistance of Heinz Funk of the Hamburg Radio Studio have brought out the Sennheiser Sound Effect Vocoder VSM 201 (see photo 5). The latest development is a smaller version of the EMS Vocoder, called the EMS 2000 (see photo 6), which, by virtue of its size and extreme portability, is particularly suited for live work.

Speech-synthesis and Vocoding
As mentioned above, a fundamental feature of vocoders is their ability to analyse and electronically simulate the sound of speech. Thus before going on to examine the operating principles of a vocoder it is first necessary to take a look at the basic characteristics of human speech.

Speech sounds
At the moment it is virtually impossible to create a realistic replica of the human voice, since not only do speech sounds have a very irregular intensity, but they are also extremely rich in harmonics. Synthesised speech is always too ‘clean’, too free from natural imperfections.

Speech itself is composed of two main component sounds:

- Air from the lungs can be forced between the vocal chords situated in the windpipe, causing these chords to vibrate and a pulsating air-column to enter the mouth and nasal cavities. The fundamental frequency of the resultant note is determined by the length, thickness and tension of the vocal chords. Sounds produced in this fashion e.g. the vowels, are known as VOICED sounds.
- Alternatively, if the air from the lungs is not forced through the vocal chords, but simply expelled through the mouth, then so-called UNVOICED sounds are produced, such as ‘f’ or ‘h’. These are basically similar to the type of sounds which can be produced by a noise generator. In the case of both voiced and unvoiced sounds the shape of the mouth and nasal cavities determines the character or timbre of the sounds. Variation of

An orchestra suddenly begins to recite a passage of Shakespeare, an electric guitar reads the news, the voice of a talker unexpectedly changes sex, a single voice sounds like a chorus — these are just a few of the amazing effects which can be obtained with a new electronic instrument — the vocoder.

This article explains the ins and outs of this fascinating new development in the field of electronic ‘music’.

C. Chapman

The author and editor wish to thank Mr. Orr of EMS Ltd., Mr. Buder of Sennheiser and Mr. Funk of the Hamburg Radio Studio for their assistance in the preparation of this article.
vocoders

Figure 1. This simplified diagram shows the basic operating principle of all vocoders. The input speech signal is analysed to provide a set of data which is used to impose the pattern or articulation of the speech signal upon an external replacement signal input. The fact that the original speech sounds are encoded in the form of control voltages gives the vocoder its name (VOICE CODER).

Figure 2. A spectrum analysis of the sound of vowels and consonants spoken by a female (figure 2a) and a male (figure 2b) voice. The pitch is the same for all the vowels. The fundamental frequency of the male voice is approx. 140 Hz, whilst that of the female voice is roughly 280 Hz. The sound produced by the vibration of the vocal chords is extremely rich in harmonics. The variation in the dynamic amplitude characteristics of different vowels is the result of the different resonances formed by varying the position of the tongue, teeth and lips, and hence the shape of the nasal and mouth cavities. This process, which amounts to a sophisticated 'filtering' of the speech sounds, is just as important in the case of unvoiced sounds. This is evident from the differences in the spectra of the two sounds 'f' and 'sh'.

cavity RESONANCES by movement of the tongue and lips controls the harmonic content of the voice and enables us to form separate vowels and consonants (see figures 2a and 2b). The lips play a particularly important role in sounds which are distinguished by their dynamic amplitude characteristics, such as the percussive attack transient of the 'p' in 'paper'.

Thus the voice can be seen as a complex sound generating instrument, consisting of a frequency and amplitude-controlled oscillator (the vocal chords and lungs), a
Speech-synthesis
Viewing the voice in this way naturally leads one to speculate whether it might be possible to synthesise speech, using techniques similar to those employed in a music synthesiser. The vocal chords could be replaced by an oscillator, the output waveform of which is sufficiently rich in higher harmonics to allow differentiated filtering, whilst a noise generator could be used to provide the unvoiced sounds. A switching circuit would cut back and forth between the above two sound sources depending upon which mode of voice was required. However problems begin to arise when one considers the type of filters that would be needed for a speech synthesiser of this type. Since the continual variation of both the static harmonic content and dynamic characteristics of the sound is crucial for the formulation of articulate speech, an equaliser-type filter system would be necessary to simulate all the nuances in the tonal character of human speech. What is more, the filter system would have to be voltage controlled if it were to have any chance of matching the rapid change in the harmonic content of speech. At this point it becomes clear that an analogue speech-synthesiser of this kind would require an enormous amount of hardware, for how does one generate the extremely complex pattern of voltages needed to control the filter bank?

One possibility to simplify the process is a hybrid system, using a memory to store the control voltages. The quality of modern speech-synthesisers which use such a system is fairly good. Doubtless many readers will have seen or heard of so-called ‘talking’ computers, which use synthetically-generated speech to express the results of the calculations, and the ‘talking’ calculator shown in photo 1 proves that it does not require an enormous amount of hardware to synthesise speech digitally. Photo 2 shows that the digital speech-synthesiser consists of just two ICs mounted on a single board. The speech components are stored digitally in a ROM, where they can be scanned by a speech synthesiser micro-controller. A D/A converter in the micro-controller then generates the analogue speech components, from their digital equivalents.

Vocoding
Although storing the speech components digitally represents by far and away the simplest solution for systems designed to generate speech (assuming the desired vocabulary is not too large), this is not the case with vocoders, and here we come to the basic difference between vocoders and speech-synthesisers.

A vocoder is basically designed to superimpose the pattern of spoken words onto a recorded non-speech signal (such as, music, the sound of wind, surf, etc.) so that the resultant effect is that of a talking orchestra, for instance. The articulation of the output signal is extremely good, being distinguished by remarkable clarity and distinctiveness. This quality of articulation, among other things, is what distinguishes the vocoder from other less sophisticated special effect devices such as the well-known WAWA pedal, or the more recent MOUTH BAG or MOUTH TUBE (see photo 3).

The latter is basically a crude acoustic-mechanical vocoder. The signal from an electric guitar or similar source is fed to a powerful amplifier, which drives a loudspeaker situated in a closed box. The amplified sound from the guitar is then fed via a plastic tube to the mouth of the musician. Without using his vocal chords, but simply by altering the shape of his mouth cavity he can then articulate the guitar signal, so that the guitar

[Image of speech synthesis diagrams]
appears to be 'talking'. This signal is picked up by a microphone in front of the musician's mouth and fed through the PA system in the usual fashion. The sounds produced by the mouth tube are essentially similar to those produced by a vocoder. However, not only is the mouth tube fairly limited in the number of possible applications, but, compared with vocoders, the quality of articulation is considerably inferior. In particular, it is extremely difficult to produce unvoiced and plosive sounds.

Modern Vocoder

By now the reader should have gained a good idea of the basic principles of vocoding: the vocoder modulates the articulation of speech upon a second 'excitation' signal. This is done by converting the input speech signal into data which can be used to vary the output signal.

Although in principle there are various different ways of analysing and synthesising speech, the three vocoders described above are all 'channel vocoders'. Figure 3 shows the functional block diagram of this type of vocoder. The speech signal (from the microphone) is fed to a bank of bandpass filters, which split the signal into a number of separate and very narrow frequency bands. By rectifying and feeding these signals through lowpass filters, a series of DC voltages which match the envelope of the filter output signals can be obtained. These are in fact the control voltages which will control the synthesiser filter bank, and represent a real...
Figure 3. Functional block diagram of a channel vocoder. All vocoders which are intended for musical and special effect applications conform to this design. A real time spectrum analysis is made of the speech signal by a bank of bandpass filters and envelope followers. The result of the analysis is a series of control voltages which drive a bank of VCAs (voltage controlled amplifiers), to vary the replacement signal. Thus the spectrum of the original speech signal is imposed upon the 'excitation' (normally non-speech) signal. The voiced/unvoiced detector continuously samples the speech signal and decides whether, at any given moment, the noise generator need be switched into circuit. The noise generator is required since most excitation signals do not have a sufficiently broad spectrum to allow the synthesis of sibilants. For the sake of simplicity only three channels are shown in the diagram.

Photo 1. Approximately 2 years ago a 'talking' calculator, which contained a very small speech synthesiser, appeared on the market.

Photo 2. The printed circuit board of the speech synthesiser inside the 'talking' calculator. The circuit consists of only two ICs: a ROM which stores the speech components in digital form, and a micro-controller which selects the components for any desired word and, by means of a D/A converter, fits them together to form an analogue speech signal.

Photo 3. An example of a mouth tube or mouth bag. The box contains a power amplifier and loudspeaker. The resultant sound is fed via the plastic tube into the mouth of the musician who then modulates or 'articulates' this signal by changing the shape of his nasal and mouth cavities. Thus he appears to make his guitar, or whatever instrument he is playing, speak or sing.

Photo 4. The full-size EMS vocoder was the first commercially available vocoder which was specially designed for musical or special effect applications in the recording studio. The instrument contains several additional features such as a pitch extractor (pitch-voltage converter) and two synthesiser VCOs which can be played on external keyboards.

time spectrum analysis of the speech signal.

The input speech signal is also fed to a second circuit, the voiced/unvoiced detector. This continuously samples the speech signal to decide whether it is a voiced or unvoiced sound, and indicates the result by switching to one of two voltage levels (e.g. 0 V and +5 V). The outputs of the voiced/unvoiced detector and the envelope followers control the synthesiser section of the vocoder. This contains the same number of filters as the analyser section, so that the excitation signal (be it simply the synthesiser oscillators and noise generator, or these two sound sources plus an external input) is analysed into the same number of separate frequency bands as the speech signal. Via a series of voltage controlled amplifiers, the outputs of the filter sections are then varied by the control voltages derived from the envelope followers, with the result that the spectrum of the speech signal is imposed upon the excitation signal.

The separate channels are summed and fed to the output stage. The resultant signal possesses the 'voice' of the excitation signal (e.g. a violin), but has the articulation of the passage of speech.

Furthermore, both the typical character of the excitation signal as well as all the nuances of articulation in the speech signal (dialect, emphasis etc.) are completely preserved. That is to say, the human voice is simply replaced by that of whatever instrument is used for the excitation signal.

In theory, therefore the voiced/unvoiced detector should be superfluous, however most excitation signals do not have a sufficiently wide dynamic spectrum to synthesise the sound of sibilants ('s', 'h', etc.). For this reason the voiced/unvoiced detector ensures that the noise generator provides the synthesiser section with the appropriate 'raw material' whenever the excitation signal cannot do so.

Photos 7a and 7b show examples of typical signals which appear at the test points numbered in figure 3. The progression of signals in photo 7a illustrates how the input speech signal is converted in the analyser section into the control voltages which command the VCAs. Photo 7b shows how the output signal is synthesised, using a generator as the excitation signal.

The second part of this article will contain a more detailed description of
how a vocoder works, and will also take a look at the various applications of vocoders.

References:
Figures 1, 2 and 3, photos 5, and 7: Sennheiser-Electronic, Wedemark, Hannover, West Germany.
Photos 1 and 2: Silicon Systems Inc., Irvine, California
Photo 3: Electro-Harmonix, New York
Photos 4 and 6: EMS, London

Photo 5. The Sennheiser Sound Effect Vocoder VSM 201. This vocoder was designed specifically for use in the studio, and can be incorporated as a module into Moog studio syntheses.

Photo 6. The 'mini' EMS vocoder; its size, price and extreme portability make it ideally suited for live stage work.

Photo 7. These photos show the type of signals which typically appear at the points numbered in figure 3.
1 Microphone (speech) signal. The trace is that of the vowel 'a' in the test word 'bast'.
2 The output signal of a filter channel in the analyser section (centre frequency 680 Hz, 6 dB bandwidth 140 Hz).
• The signal after rectification.
• The control voltage obtained after the rectified signal has been 'smoothed' by the lowpass filters.
• The excitation signal from a pulse generator. The frequency is approximately 150 Hz.
• This signal is obtained after the pulse signal has been fed through the synthesiser filters.
• This is the signal which is obtained once the output signal of the analyser section (centre frequency 680 Hz, 6 dB bandwidth 140 Hz) has been modulated onto the output of the synthesiser channels. The similarity of this signal with that of the original speech signal can be clearly seen.
This final part of the Formant series completes the description of the synthesiser by describing the COM (control and output module) and by giving an overall wiring diagram. Possibilities for further expansion of the system are also discussed.

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The COM contains a tone control amplifier with bass, middle, treble and volume controls, and an output buffer capable of driving high impedance (> 600 Ω) headphones for monitoring or practice purposes. The COM front panel also contains the indicator LEDs for the three power supply voltages and the gate signal. These indicators should not be regarded merely as a gimmick but as an important aid to monitoring the state of the Formant system. A fault in any of the supply voltages is immediately indicated by one of the LEDs, as is the absence of a gate pulse.

COM circuit
The complete circuit of the COM is given in figure 1a. The input signal is fed to a volume control P1a and thence to an 'anti-pop' filter built around A1. This is a 12 dB/octave highpass filter with a break frequency of around 20 Hz. It suppresses low-frequency transients and rolls off the bass response of the system to reduce 'listener fatigue' which can be caused by the low bass notes of electronic music, especially with full bass boost. By rolling off the bass response the filter also helps protect the bass drivers of the loudspeakers against excessive, very low-frequency signals. Indeed, if the synthesiser is to be used with small 'bookshelf' speakers it may be advisable to raise the turnover point of the filter to 40 Hz by changing the value of R1 and R2 to 39 k.
The treble and bass controls, built around A2, are a conventional Baxandall network. To avoid the middle control interacting with the bass and treble controls it is constructed separately around A3. The output of A3 then feeds into a second volume control P1b. The use of a ganged volume control on a single signal channel may seem a little unusual, but it does have several advantages. A volume control at the input to the COM prevents any possibility of overloading A1, whatever the signal level. On the other hand, the provision of a volume control later in the circuit allows a better signal-to-noise ratio to be maintained at low settings of the volume control, since noise (principally from A1) is attenuated along with the signal as the control is turned down. The fact that this control produces a 'double logarithmic' characteristic does not cause any inconvenience in operation.

No power amplifier is built into the COM as the heat generated in the output stage could cause temperature drift problems in other circuits in the system. However, the COM is provided with an internal output to a separate power amplifier, IOS. The output of the amplifier may then be brought back through the COM via the PA input connection on the COM board edge connector to a socket on the COM front panel (OUT 2). The COM output is itself also brought out to a socket on the front panel (OUT 1) into which high impedance headphones may be plugged. Note that a 6.3 mm jack socket is used for OUT 2.
The four indicator LEDs also receive their power via the COM edge connector from the appropriate circuits, and are also mounted on the COM front panel.

Construction and testing of the COM
A printed circuit board and component layout for the COM are given in figure 2, a front panel design is given in figure 3 and wiring to front panel mounted components is shown in figure 4. Screened leads should be used for the connections to bass, middle and treble potentiometers B, M, and T.

Some readers may not wish to bring the output of a power amplifier back through the COM to output 2, since this may not be convenient especially if the synthesiser is to be used with, say, an existing hi-fi setup. In this case two options are open. Output sockets 1 and 2 can simply be connected in parallel or alternatively output socket 2 can be wired direct to input IS to provide an output signal unaffected by the tone and volume controls.

It is not intended to provide a design for an output power amplifier since several good designs have already been published in Elektor. However, a few hints on the mounting of such an amplifier will not go amiss. As mentioned earlier,
the power amplifier should not be mounted in a plug-in module since it may then cause thermal problems. It should preferably be mounted at the back of the module cabinet with the output transistors mounted on heatsinks whose fins are external to the module housing. The Formant power supply is not intended to supply current for a power amplifier, so a separate power supply will be required. The mains transformer should be mounted as far away as possible from the Formant modules to reduce hum pickup (the same applies to the Formant mains transformer).

The COM can be tested by feeding in a signal from one of the VCOs and monitoring it on an oscilloscope to check that the waveform is undistorted. The gain of the COM output stage, A4, can be varied between about 1.8 and 11 by means of PS. This preset should be adjusted so that full drive of the headphones or power amplifier is obtained with the volume control turned fully up (clockwise).

### Patchcords

Due to the hardwired interconnections between modules, Formant is perfectly playable without any of the front panel patching sockets being used. However, for effects such as vibrato and tremolo, patchcords are used to connect the outputs of the LFO module to the VCOs or VCA. These are very easy to make. A
Parts list for figures 1 and 2.

Resistors:
- \( R_1, R_2 = 82 \, k \)
- \( R_3, R_8, R_{18} = 470 \, \Omega \)
- \( R_4, R_6 = 1 \, k \)
- \( R_5, R_7, R_{11}, R_{13} = 6k8 \)
- \( R_9, R_{14} = 3k9 \)
- \( R_{10}, R_{12} = 100 \, k \)
- \( R_{15}, R_{17} = 220 \, k \)
- \( R_{16} = 22 \, k \)
- \( R_{19} = 4k7 \)

Potentiometers:
- \( P_{1a}, P_{1b} = 4k7 \) log ganged pot.
- \( P_2, P_3, P_4 = 100 \, k \) lin.
- \( P_5 = 220...270 \, k \) preset.

Capacitors:
- \( C_1, C_2, C_9 = 100 \, n \)
- \( C_3, C_4 = 10 \, n \)
- \( C_5, C_6 = 39 \, n \)
- \( C_7 = 15 \, n \)
- \( C_8 = 3n3 \)
- \( C_{10}, C_{11}, C_{12} = 680 \, n \)

Semiconductors:
- \( IC_1 = 4136 \) (DIL package) EXAR, Fairchild, Raytheon or Texas.

Miscellaneous:
- 31-way connector to DIN 41617
- 3.5 mm jack socket
- 6.3 mm jack socket
- 4 collet knobs, 13...15 mm diameter, with pointer.
Figure 3. Front panel layout for the COM (EPS 9729-2).

Figure 4. Wiring diagram for the front panel mounted components.

Figure 5. Inter-module wiring for the basic Formant system. Supply voltage connections have been omitted for reasons of clarity. The LFO and noise modules have been omitted as the only hardwired connections they have are supply connections.

Figure 6. The ‘gate-LED’ output of the interface receiver can be simplified by mounting R30 in the ‘D4’ position.

Flexible single-core cable of about 30 cm length is fitted with a 3.5 mm jack plug at each end. The cable is soldered to the centre contact (ball) of the plug, no earth connection being necessary as the earth return is made through the internal module wiring. In the interests of long life the patchcord wire should not be too thin, and some sort of strain relief should be used where the wire enters the plugs. About a dozen patchcords should prove sufficient for most applications. Alternatively, to keep the front panels more tidy the patchcords can be made in several different lengths, each designed for an interconnection between two specific modules. Different colours of wire may also be used to simplify checking of complicated patch connections.

Front panels
As each module was described, a suitable front panel layout was also given. It has now been decided to make these panels available through the EPS printed circuit board service. As shown in figure 7, the pre-drilled metal boards are sprayed matt black, and the legends and scales are printed in white. Experiments have shown that this combination
provides good legibility even under extreme lighting conditions. Further details are given in this month’s EPS list.

Extending Formant

Although the Formant system so far described is a versatile instrument giving performance comparable to commercial designs at a greatly reduced cost, it is nonetheless relatively unsophisticated compared to the larger commercial instruments. However, because of the modular construction it is a simple matter to extend the system. Quite a lot can be accomplished simply by adding more of the modules already described, for example extra VCOs, VCFs and VCAs, to obtain a more varied sound. Many effects however, require the addition of completely new modules and ancillary circuits, some of which it is hoped will be discussed in future issues of Elektor. One possibility which can be implemented immediately is the addition of the Elektor equaliser (January 1978) to allow presettable tailoring of the synthesiser spectrum. The equaliser p.c. board is of Eurocard format, compatible with the other Formant modules. Another module which it is hoped to feature, which will greatly increase
the tone colour possibilities of the system, is a 24 dB/octave VCF module. Banks of resonant filters are also a useful addition to the tone-forming capabilities of the synthesiser, especially for the production of vocal-type sounds. These are not voltage-controlled filters, but have manually presettable centre frequency and Q factor.

Phasing circuits are frequently used in synthesizers, and are particularly useful for more realistic reproduction of string tones. Another tone modifying circuit which is often used is the ring modulator. This circuit produces the sum and difference of two input frequencies at its output. The frequencies produced are not necessarily harmonically related, and the sound is not particularly ‘musical’; however, the ring modulator is extremely useful for special effects such as bells, gongs and cymbals.

In its basic form the range of expression available from the synthesiser is somewhat limited by the fact that it is played by a keyboard. However, there are various ways in which this can be remedied. The addition of a ‘pitch-bender’ joystick, which feeds a manually controllable DC voltage to the VCOs, allows modulation of the pitch of a note by hand in much the same way that a guitarist ‘pulls’ the strings of his guitar.

An interesting possibility is the elimination of the keyboard by playing the synthesiser via another instrument. This is accomplished by the use of a pitch-to-voltage converter, which produces an output voltage proportional to the pitch of the control instrument. This in turn controls the frequency of the synthesiser VCOs. An envelope follower produces an output voltage which follows the control instrument’s amplitude, and this is used to control the gain of the VCA. The result is a synthesiser sound which has the dynamics of the original instrument.

Other useful additions to the synthesiser system are sequencers, sample-and-hold circuits and reverberation/echo units. Sequencers are used to store (either by analogue or digital means) a sequence of VCO/VCF control voltages. These are then ‘played back’ into the synthesiser automatically to generate a note sequence which can, for example, be used to provide the backing for a manually played melody.

A sample-and-hold circuit is frequently used to take sequential samples of the instantaneous voltage of a sawtooth waveform. This sequence of voltage samples is used to control the synthesiser to generate a pseudo-random sequence of notes.

Reverberation units are used to enhance the somewhat ‘dry’ sound of the synthesiser by allowing notes to die away gradually rather than be cut off abruptly when a different key is pressed. Such units may contain mechanical delays such as plates or springs, or purely electronic delays such as analogue shift registers may be employed.

Loudspeakers
Before concluding this article a few words on the choice of loudspeakers for use with Formant will not come amiss. Readers building a synthesiser for home use will probably wish to play the instrument through an existing hi-fi setup, at least to begin with. If this is the case care should be taken not to overload the loudspeakers, by keeping the volume fairly low. Hi-fi loudspeakers are designed to handle a much more broadly distributed power spectrum than that produced by a synthesiser, and it is quite easy to damage the tweeters with a sustained high frequency note.

For serious use a purpose-designed loudspeaker system should certainly be considered. Horn systems are to be favoured because of their high efficiency and a dealer who specialises in electronic music systems should be able to offer advice on suitable loudspeakers.
Many hi-fi enthusiasts may not realize that significant distortion may be introduced into an audio signal by the connections between the amplifier output and the loudspeakers. In the first place, output current from the amplifier has to travel across several non-soldered metal-to-metal contacts, for example plug and socket connections at the amplifier output and the loudspeaker inputs, and loudspeaker switches within the amplifier (of which more later). For minimum distortion these contacts should not only have a very low resistance, but must also have a constant, linear resistance.

Oxidation of the metal surfaces of plugs, sockets and switch contacts can produce a non-linear resistance which varies with the current flowing through it, thus distorting the signal fed to the loudspeakers. DIN loudspeaker plugs and sockets are particularly bad in this respect due to their very small contact area, and should be avoided. Where non-soldered connections must be made the use of screw terminals or robust 4 mm 'banana' plugs and sockets is to be preferred.

The second area which can cause degradation of the audio signal is the connecting cable itself. When a loudspeaker is being driven by an amplifier the loudspeaker cone should move exactly in sympathy with variations of the amplifier output voltage. Ideally, if a loudspeaker is fed with, say, a step input, the cone should move quickly to the appropriate position and stop. In practice, of course, this does not happen. A loudspeaker possesses inertia and compliance, so that the cone will tend to oscillate about its final position before settling down. Whilst this 'ringing' is in progress the loudspeaker acts as a generator and tries to pump current back into the amplifier output. If the amplifier output impedance is low (and it generally is) the loudspeaker sees a short-circuit and the cone movement is quickly damped by electromagnetic braking. The 'damping factor' of an amplifier is defined as the ratio of the load impedance to amplifier output impedance. As the output impedance of a modern transistor amplifier is generally a fraction of an ohm, damping factors are typically between 50 and 200 with an 8 ohm load. However, the resistance of the loudspeaker connecting cable appears in series with the amplifier output and must be considered as part of the amplifier output impedance. If the loudspeaker cable is thin its resistance will be high and the damping factor will be considerably reduced. In addition, some of the amplifier's output voltage will be dropped across the cable resistance rather than appearing across the loudspeaker.

Thus the second rule when connecting loudspeakers is to use heavy-duty cable. Fuses, which are sometimes inserted in series with amplifier outputs for loudspeaker protection, should also be avoided since they can have a significant resistance.

Recent research, particularly by Japanese manufacturers, seems to indicate that the inductance of loudspeaker cables has a significant effect on transient response, and Hitachi, JVC, Pioneer and Sony are all introducing special loudspeaker cables which are claimed to give an improved sound. Whether or not these claims are true is still a matter for conjecture.

Returning to the subject of loudspeaker switching, figures 1 and 2 show two typical switching arrangements which allow two sets of speakers to be connected to an amplifier, either independently or simultaneously. One channel only is shown and the circuits are identical for the other channel. Although such switching arrangements offer convenience of use, they may not be such a good idea from a sound quality point of view due to the contact resistance of the switches. If loudspeaker switching is employed in an amplifier then the switches used should be rated at several amps to ensure minimum contact resistance.

Both the switching arrangements shown in figures 1 and 2 have their advantages and disadvantages. In figure 1 both speakers appear in parallel across the amplifier output in the A + B position. Whilst this does mean that the damping factor is maintained the reduced load impedance can cause overloading.

In figure 2 the speakers are connected in series in the A + B position. Assuming that both speakers have the same impedance this connection, of course, doubles the load impedance, so there is no risk of overload. However the available output power is halved (since \[ P = \frac{U^2}{2R} \]) and the damping factor is reduced to less than unity, since each loudspeaker has the other in series with it as a source impedance.

In conclusion, anyone contemplating the building of an audio amplifier and/or loudspeakers would be well advised to bear in mind all the points raised in this article. To summarise:

1. Connection to the loudspeakers should be made with the minimum number of non-soldered connections (plug and socket connections and switches) in series with the signal path.
2. The cable to the loudspeakers should have as low a resistance as possible. Fuses in series with the loudspeakers, although seemingly desirable from a circuit protection point of view, have a detrimental effect on sound quality and should be avoided.
16 segments

The entire alphabet from A to Z, all digits from 0 to 9, plus, minus, equals and summation signs and a whole series of other symbols may be depicted by a 16-segment display, which Siemens is now putting on the market under the designation IA 4041. This LED display offers an alphanumeric set comprising 64 characters each four millimeters high. Four such displays are combined on one module with the associated electronics. The modules can be arranged in rows of practically unlimited length.

The so-called 7-segment displays with three horizontal and four slightly sloping vertical bars are well-established in a wide field of applications ranging from measuring instruments to TV sets and watches and clocks of all sizes. Liquid crystals and oblong light-emitting diodes are equally suitable as the display medium. However, conventional 7-segment displays essentially provide for the ten digits only.

A very significant feature is compatibility with microprocessors, which could now learn to talk with the aid of the 16-segment displays – an economically unjustifiable proposition so far. The alphanumeric character set permits the display of operating states and program progress. A related application would be in keyboard stations or phototypesetting equipment, where the typed information could be displayed for checking purposes before it is printed.

Each of the four display units of a module puts out 0.1 med per segment with a viewing angle of 20° from all sides. Up to 16 displays (four HA 4041 modules each with a width of 25 mm) may be lined up as an array, while more than 16 displays can be combined with modest circuit requirements. The module packages are designed to present an evenly spaced display, also when used in arrays.

Siemens AG, Postfach 103, D-8000 München 1, Federal Republic of Germany

Dot matrix printer

A range of compact dot matrix impact printers, the 7040 series, has been introduced by Implectron Limited. Suitable for a wide range of data output applications such as point of sale documentation and data logging, the low cost range features ease of operation, compact size and simple interface circuitry.

The printer utilizes a serially driven print element consisting of 7 print solenoids and associated print wires. The wires are arranged in a vertical line and driven horizontally across the paper at constant speed. Print speed is over one complete 3.3" line per second, and each line contains 40 characters. Character height is 0.123 inches. By use of external control circuitry, the printer may produce characters of almost any density or font desired. Because the print head travels at constant speed, there is no need for a complex feedback system to determine the correct timing of print pulses. Ribbon feed, ribbon reverse (and in some cases paper feed) are controlled automatically without control signals.

Unlike many printers, the 7040 series has no clutches, timing discs or reversing mechanisms to control print head movement. The head always travels a complete line from left to right and then returns to its home position regardless of the number of characters printed on each line.

The range has been designed to produce up to 5 copies of the top copy, depending on paper thickness and type. Maximum paper thickness is 0.015" overall.

Two models are currently available from Implectron. The basic model 7040 is a simple printer with no paper supply or document handling mechanisms. Optional extras do however include paper roll holder, journal take up and assembly, or secondary motor for high speed paper feed.

A more sophisticated variation, the Model 7040T, is arranged in a flat bed document printer configuration. As documents are inserted for printing, a solenoid-activated roll clamps the document, permitting proper feeding and preventing accidental or premature removal. This model also features a highspeed document feed of 10 lines per second. Optional features of the 7040T include reverse document feed and top of form sensors.

Specification:

- Speed: 1.04 lines/second
- Character Height: 0.123 inches
- Data Input: Synchronous
- Line Length: 3.3 inches
- Print Solenoid Power: 40 V (DC) ± 10% @3.6A peak current per solenoid.
- Average current approx. 0.87A for 1.5 ms cycle time.

Implectron Limited, Implectron House, 23-31 King Street, London W3 9LH, England

Remote control chips

AMI Microsystems have introduced a 31-command remote control chip set with keyboard inputs, oscillators, and both analog and digital receiver output all on board the chip.

Consisting of an S2600 transmitter and an S2601 receiver, the set reduces the part count for TV equipment designed for remote control via radio frequency, infrared, ultrasonic or hardwire transmission media. Among the applications for the devices are motorized toys such as trains and boats, home security systems, automatic telephone calling equipment, industrial controls, TV and stereo controls, and traffic controls for emergency vehicles.

The AMI S2600 and S2601 have eliminated the need for external crystals; only a resistor and a capacitor are required externally for a frequency reference. The S2601 receiver will tolerate up to ± 24% difference in the timing frequency and still operate. However, the circuit has a very high immunity to noise or spurious commands.

Squiggly command rejection has been achieved through a 5-bit command code system which requires that identical, proper commands be transmitted twice in succession before the receiver issues an output. In addition, a correct five-bit fixed (mask-programmable) preamble code must be received.

Eleven outputs (six digital, three analog, a pulse train and an on/off) are available from the receiver. Five binary outputs present the five-bit code received, while the sixth digital output is a "data valid" signal. The pulse train is useful for indexing a stepping switch, as in TV channel selection, or operating a stepping or counting device in industrial controls or toys. The on/off output can be used to remove and restore the main power supply. The analog outputs can independently provide up to 64 distinct DC levels for controlling motor speed, volume, brightness, or similar electronic settings; one of these analog outputs is mutable and can be used for TV sound control.
The S2600 transmitter is a low power drain CMOS chip (dissipating only 20 mW) with an on-chip oscillator, 11 keyboard inputs, a keyboard encoder, a shift register and control logic. Its output is a 40 kHz square wave which is pulse code modulated. The S2600 can transmit a 12-bit message including sync frame, preamble, 5-bit command code, and end of message bits every 38.4 milliseconds. The S2601 receiver is a P-channel MOS chip with on-chip oscillator, five keyboard inputs, a 40 kHz signal input, decoding logic and eleven outputs. Its on-chip memory saves received commands and the logic compares them with later receptions. If the codes do not match, the receiver saves the last code received for its next comparison try. When two successive identical codes are received, a valid output is issued.


Digital inductance meter

AIM Cambridge Ltd is pleased to announce a new, low cost Automatic Digital Inductance Meter type DLM307. This instrument, intended as a complement to the Digital Capacitance Meter DCM302, is fully auto-ranging and will measure up to 1.999 H full scale, whilst the most sensitive range has a resolution of 1 μH. The readout is a 3½ digit LED display and the unit can be powered either from batteries or a small mains power unit, both of which are supplied. As in AIM’s Digital Capacitance Meter, the unit has no operator controls apart from a touch-pad which is used to turn on the instrument for about 10 seconds. The correct measurement range is found automatically within 2 seconds of switch-on, after which measurements are repeated every 0.4 seconds.

The measurement technique employs a highly linear L-R oscillator whose period is proportional to the value of the inductor being measured. This period is then measured using digital techniques employing CMOS integrated circuits. One advantage of this approach is that the measurement frequency is appropriate for the value of the inductor being measured. For example, large value inductors are measured at frequencies between 25 Hz and 250 Hz whilst small inductors are measured at frequencies up to 1 MHz.

AIM Cambridge Limited, Edison Road, Industrial Estate, St. Ives, Huntingdon, Cambs. PE17 4LF England.

Microwave spectrum analyser

The new 7L18 microwave spectrum analyser from Tektronix incorporates several advanced technological innovations to offer a combination of exceptional performance and ease of operation. A high-stability phase-lock system yields a resolution of 30 Hz at frequencies up to 12.5 MHz, while external waveguide mixers extend the overall frequency range up to 60 GHz. Other important technological developments used in the 7L18 include microprocessor-aided controls for ease of operation and adjustment, a split digital-memory system, and YIG tunable filters for spuriously-free display from 1.5 MHz to 18 GHz. The 7L18 is a three-module wide plug-in unit for the Tektronix 7000 Series modular instrumentation range. With a direct coaxial input it will display the spectrum of signals from 1.5 to 18 GHz, with a resolution of 30 Hz up to 12.5 GHz.

The new external waveguide mixers extend the frequency coverage to 60 GHz with a response flatness specified at ± 3 dB or better. Hence relative amplitude measurements can be made with confidence when operating with waveguide mixers. In addition, the built-in preselector system is fully characterized for absolute amplitude measurements up to 18 GHz.

Measured in terms of residual frequency modulation, the stability resulting from the new phase-lock circuitry is specified as 10 Hz or less up to 4.5 GHz (about four parts in 10⁶). Digital storage provides flicker-free displays at the lowest sweep speeds, fine detail and unlimited storage time for subsequent viewing, comparison or easy photographic recording. A split memory allows comparison of a reference with an existing spectrum or a calculated display of the difference between two spectra. The storage circuitry also includes a maximum-hold capability that allows monitoring of frequency or amplitude signal variations.

A microprocessor provides automatic resolution and sweep time/division modes to optimize setting up the display and prevent many potential operator errors. In the non-auto mode of operation, any combination of control settings which results in an uncalibrated display also turns on the ‘un calibrated’ indicator light. The 7L18 spectrum analyser is easily transportable, and applications include microwave-relay and satellite communication, frequency management and microwave component and system manufacture.

The instrument can also be converted to a high-quality microwave receiver for time-domain measurements by setting the frequency span to zero and using the calibrated time base.


(717 M)
P.C.B. KIT
Mega Electronics Ltd, introduced a comprehensive kit which enables the preparation of artwork for, and the production of, both printed circuit boards and boards and front panels or labels.

Known as the Photolab Kit, it consists of an ultraviolet exposure unit, drafting aids and film, positive resist coated epoxy glass laminate sheets, developing and etching trays, label and panel materials, high-speed drill, and all the requisite developers. The Photolab Kit has been designed for use by both the hobbyist and the professional engineer. It has been introduced to fill the gap between commonly used 'off-the-shelf' prototype p.c.b. production methods and the facilities offered by the existing, larger kits currently available. It is priced at only £44.50, complete, and can handle p.c. boards and labels of up to 9 x 6 in.

Mega Electronics Ltd, 9, Radwinter Road, Saffron Walden, Essex CB1 3HU, England

(682 M)

µP based analyser
The 7LS from Tektronix U.K. Ltd, is a microprocessor-based spectrum analyser that achieves exceptional frequency accuracy (two parts in 10¹¹) through a unique combination of synthesiser and digital technology. The inherent stability of the synthesiser method used, coupled with digital tuning techniques, means that the centre frequency can be set with 6-digit accuracy immediately after turn-on, with no need to fine-tune the displayed signal. The built-in microprocessor intelligence is used to simplify operation of the instrument. The instrument processes control settings, processes frequency and reference level information and optimises sweep time and resolution for the chosen frequency span. At turn-on, the 7LS is preset to a reference level of +17 dBm and a centre frequency of zero, which provides not only input attenuation to protect the front end but also a marker to verify correct operation.

The 7LS spectrum analyser has a full 80 dB spur-free dynamic range for measuring wide relative amplitudes. Nanovolt sensitivity allows very low-level signals and noise to be measured. A front-panel input buffer control greatly increases front-end immunity to intermodulation, maintaining a constant reference level.

The instrument is fully calibrated in dBm, dBV or volts per division. The reference level can be set in 1 dB steps, eliminating the need to interpolate amplitude levels. To accommodate a wide variety of input impedances, the 7LS uses plug-in modules. Three standard modules offer 50 Ω, 75 Ω and 1 Ω, and special modules for other impedances can be provided. The 7LS incorporates a digital storage and averaging technique. The entire display is stored electronically and updated during each sweep, and two complete displays can be held in the memory for comparison. Two display modes are available: a conventional peak display or a digitally averaged display. For special measurements, such as signal/noise ratio, these two modes can be used simultaneously by setting the continuously adjustable peak/average threshold. A 'maximum hold' control enables maximum signal levels to be stored for checking long-term amplitude and frequency drifts. Options available for the 7LS spectrum analyser include a tracking generator, logarithmic frequency display and front-panel readout unit.

Tektronix U.K. Ltd., Beaverton House, P O Box 69, Harpenden, Herts, England

(678 M)

Chiming annunciator
A new chiming audible has been added to the Highland range of audible warning devices. The repeating chime has a frequency of 2900 Hz ± 500 Hz working at 6...16 V DC.

Maximum current used at 16 V DC is 8 mA. Light in weight and very compact it is easily installed with a single 32 mm hole fixing. Overall dimensions are 42.9 mm (1 11/16") diameter at back, 47.6 mm (1 7/8") in length. It is simply connected by two screw cable connections. Chiming Sonalerts produce a unique tone by electronic means. A semi-conductor oscillator driving a piezo-ceramic transducer produces a penetrating but not unpleasant sound. The audible volume can be varied by adjusting the supply voltage.

Highland Electronics Ltd., Highland House, 8 Old Steine, Brighton, East Sussex, BN1 1EJ England

(683 M)

5 Amp negative voltage regulator
This hybrid voltage regulator, the µA79HG, is an adjustable four terminal device capable of supplying in excess of 5 A over a 24 V to −2.2 V output range. It is a complement to Fairchild's µA78HG positive adjustable regulator.

It has been designed with all the inherent characteristics of the monolithic four terminal regulator and offers full thermal overload plus short-circuit protection. Should the safe operating area ever be exceeded, the device simply shuts down. Packaging is in a hermetically sealed TO-3 can. Absolute maximum ratings include an input voltage of −40 V and internal power dissipation of 50 W at a case temperature of 125°C.

Fairchild Camera & Instrument (UK) Ltd., 230 High Street, Potters Bar, Herts, EN6 5LU, England

(681 M)

Elektor announces new logic
Beek, Limburg, 1 Apr. 1984- Elektor, one of the world's major suppliers of kits and components, today announces a new line of feminine logic which is now available from stock to Elektor readers. The first device in this new logic family is called the 'Maybe' gate. Its new logic symbol is shown here.

Elektor's new line of feminine logic functions as follows: (a) inputs 1 and/or 2 'high', may cause the output to go 'high' (but maybe not)
(b) if the output does go 'high' it will remain 'high' unless it goes 'low'
(c) if the output is 'high' and either input 1 or 2 goes 'low' the device will probably go 'low'.

Elektor can see the potential for the 'Maybe' gate in such items as 'household computers', computer-piloted automobiles and, most important of all, weather-forecasting computers.

Elektor, Peter Treckpoelstraat 2, 6191 VK Beek (L), Netherlands.

(695 M)
Wherever possible in Elektor circuits, transistors and diodes are simply marked 'TUP' (Transistor, Universal PNP), 'TUN' (Transistor, Universal NPN), 'DUG' (Diode, Universal Germanium) or 'DUS' (Diode, Universal Silicon). This indicates that a large group of similar devices can be used, provided they meet the minimum specifications listed in tables 1a and 1b.

Table 1a. Minimum specifications for TUP and TUN.

<table>
<thead>
<tr>
<th>Type</th>
<th>Uceo max</th>
<th>Ic max</th>
<th>he max</th>
<th>Ptot max</th>
<th>ft min</th>
</tr>
</thead>
<tbody>
<tr>
<td>TUN</td>
<td>20 V</td>
<td>100 mA</td>
<td>100</td>
<td>100 mW</td>
<td>100 MHz</td>
</tr>
<tr>
<td>TUP</td>
<td>20 V</td>
<td>100 mA</td>
<td>100</td>
<td>100 mW</td>
<td>100 MHz</td>
</tr>
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</table>

Table 1b. Minimum specifications for DUG and DUS.

<table>
<thead>
<tr>
<th>Type</th>
<th>UR max</th>
<th>IF max</th>
<th>IR max</th>
<th>Ptot max</th>
<th>CD max</th>
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</thead>
<tbody>
<tr>
<td>DUG</td>
<td>Si</td>
<td>25 V</td>
<td>100 mA</td>
<td>250 mW</td>
<td>10 pF</td>
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<tr>
<td>DUS</td>
<td>Ge</td>
<td>20 V</td>
<td>35 mA</td>
<td>250 mW</td>
<td>10 pF</td>
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</table>

Table 2. Various transistor types that meet the TUP specifications.

<table>
<thead>
<tr>
<th>TUN</th>
<th>NPN</th>
<th>PNP</th>
</tr>
</thead>
<tbody>
<tr>
<td>BC 107</td>
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<td>BC 108</td>
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<td>BC 109</td>
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<tr>
<td>BC 207</td>
<td>BC 383</td>
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</table>

Table 3. Various transistor types that meet the TUP specifications.

<table>
<thead>
<tr>
<th>TUP</th>
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<th>PNP</th>
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<tr>
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<tr>
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<td>BC 262</td>
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<td>BC 178</td>
<td>BC 263</td>
<td>BC 417</td>
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<td>BC 204</td>
<td>BC 307</td>
<td>BC 418</td>
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<td>BC 205</td>
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<td>BC 206</td>
<td>BC 309</td>
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<td>BC 320</td>
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<td>BC 213</td>
<td>BC 321</td>
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<td>BC 214</td>
<td>BC 322</td>
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<td>BC 251</td>
<td>BC 350</td>
<td>BC 558</td>
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<td>BC 252</td>
<td>BC 351</td>
<td>BC 559</td>
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</table>

The letters after the type number denote the current gain:
A \( \alpha' = 125-260 \)
B \( \alpha' = 240-500 \)
C \( \alpha' = 450-900 \)

Table 4. Various diodes that meet the DUG specifications.

<table>
<thead>
<tr>
<th>DUG</th>
<th>DUS</th>
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<tbody>
<tr>
<td>BA 127</td>
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<tr>
<td>BA 217</td>
<td>BAX 13</td>
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<tr>
<td>BA 218</td>
<td>BAY 61</td>
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<tr>
<td>BA 221</td>
<td>1N914</td>
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<tr>
<td>BA 222</td>
<td>1N4148</td>
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</table>

Table 5. Minimum specifications for the BC107, -108, -109 and BC177, -178, -179 families (according to the Pro-Electron standard). Note that the BC179 does not necessarily meet the TUP specification \( I_{c,\text{max}} = 50 \text{ mA} \).

<table>
<thead>
<tr>
<th>NPN</th>
<th>PNP</th>
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<td>BC 107</td>
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<td>BC 263</td>
<td>BC 263</td>
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</table>

Table 6. Various equivalents for the BC107, -108, -109 families. The data are those given by the Pro-Electron standard; individual manufacturers will sometimes give better specifications for their own products.
Pin-compatible CMOS equivalents available from Teledyne Semiconductor and National Semiconductor.
PHILTRON
Electronic Components Specialists

325, DUTOIT STREET, P.O. BOX 2749, PRETORIA,
0001 TRANSVAAL. REPUBLIC OF SOUTH AFRICA
Telegraph address "TRINITRON"

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BINDERS
PRINTED CIRCUIT
BOARDS

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Projects, data etc.

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Monsanto —
Texas — Interface —
Linear — MOS — Signetics —
Fairchild
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Tantalum
Polyester
Electrolytic
Co-axial &
P.C. Mount

Resistors

I.C.'s Op Amps
Vol. Regs.,
Lin. Amps,
Digitals, Nor,
Latch etc.

LED'S

Panel Meters

Sole South African distributors for ELEKTOR
Trade Enquiries Wel e